

**MOTOROLA  
SEMICONDUCTOR  
TECHNICAL DATA**

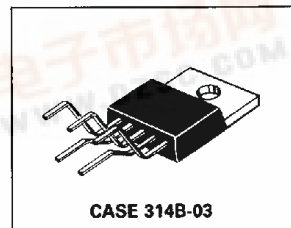
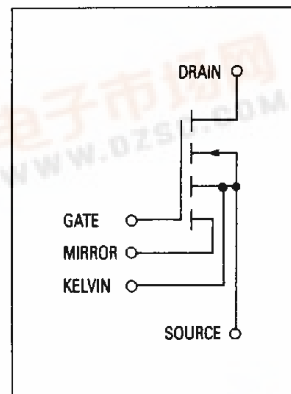
**Power Field Effect Transistor  
N-Channel Enhancement-Mode  
Silicon Gate  
with Current Sensing Capability**

**MTP30N08M**

**TMOS SENSEFET DEVICE  
30 AMPERES  
R<sub>DS(on)</sub> = 0.065 OHM  
80 VOLTS**

This TMOS Power FET with current sensing capability is designed for all power control applications where it is desirable to sense current such as in power supplies and motor controls. This device allows current sensing with a minimum of power loss.

- "Lossless" Current Sensing for Maximum Efficiency  
— Sense Current is Reduced by a Factor of 900
- Ideal for Short Circuit/Overload Protection
- Simplifies Many Circuits When Used With Current Mode Integrated Circuits Such as the MC34129
- Kelvin Source Contact to Maximize Accuracy
- Rugged — SOA is Power Dissipation Limited
- Low R<sub>DS(on)</sub> — 0.065 Ohms Maximum



**NOTES:**

1. Handling precautions to protect against electrostatic discharge is mandatory.
2. Do not use the mirror FET independent of the power FET
3. It is recommended that the mirror terminal (M) be shorted to the Kelvin Terminal (K) when current sensing is not required

**MAXIMUM RATINGS** (T<sub>C</sub> = 25°C unless otherwise noted)

Rating	Symbol	Value	Unit
Drain-to-Source Voltage	V <sub>DSS</sub>	80	Vdc
Drain-to-Gate Voltage (R <sub>GS</sub> = 1 MΩ)	V <sub>DGR</sub>	80	Vdc
Gate-to-Source Voltage — Continuous — Non-Repetitive (t <sub>p</sub> ≤ 50 μs)	V <sub>GS</sub>	±20 ±40	Vdc
Drain-to-Mirror Voltage	V <sub>DMS</sub>	80	Vdc
Gate-to-Mirror Voltage — Continuous — Non-Repetitive (t <sub>p</sub> ≤ 50 μs)	V <sub>GM</sub>	±20 ±40	Vdc
Drain Current — Continuous — Pulsed	I <sub>D</sub> I <sub>DM</sub>	30 90	Amps
Sense Current — Continuous — Pulsed	I <sub>M</sub> I <sub>MM</sub>	33 100	mA
Total Power Dissipation @ T <sub>C</sub> = 25°C Derate above 25°C	P <sub>D</sub>	125 1	Watts W/°C
Operating and Storage Temperature Range	T <sub>J</sub> , T <sub>stg</sub>	-55 to 150	°C

**THERMAL CHARACTERISTICS**

Thermal Resistance, Junction-to-Case Junction-to-Ambient	R <sub>θJC</sub> R <sub>θJA</sub>	1 62.5	°C/W
Maximum Lead Temperature for Soldering Purposes, 1/8" from case for 5 seconds	T <sub>L</sub>	260	°C



**ELECTRICAL CHARACTERISTICS** ( $T_C = 25^\circ\text{C}$ ,  $V_{MK} = 0$  unless otherwise noted.)

Characteristics	Symbol	Min	Typ	Max	Unit
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**OFF CHARACTERISTICS**

Drain-to-Source Breakdown Voltage ( $V_{GS} = 0$ , $I_D = 0.25$ mA)	$V_{(BR)DSS}$	80	—	—	Vdc
Zero Gate Voltage Drain Current ( $V_{DS} = 80$ V, $V_{GS} = 0$ ) ( $V_{DS} = 80$ V, $V_{GS} = 0$ , $T_J = 125^\circ\text{C}$ )	$I_{DSS}$	—	—	10 100	$\mu\text{Adc}$
Gate-Body Leakage Current — Forward ( $V_{GSF} = 20$ Vdc, $V_{DS} = 0$ )	$I_{GSSF}$	—	—	100	nAdc
Gate-Body Leakage Current — Reverse ( $V_{GSR} = 20$ Vdc, $V_{DS} = 0$ )	$I_{GSSR}$	—	—	100	nAdc

**ON CHARACTERISTICS\***

Gate Threshold Voltage ( $V_{DS} = V_{GS}$ , $I_D = 1$ mA) ( $T_J = 125^\circ\text{C}$ )	$V_{GS(th)}$	2 1.5	2.5 —	4 3.5	Vdc
Static Drain-to-Source On-Resistance ( $V_{GS} = 10$ Vdc, $I_D = 15$ Adc)	$R_{DS(on)}$	—	0.05	0.065	Ohms
Drain-to-Source On-Voltage ( $V_{GS} = 10$ Vdc) ( $I_D = 30$ A) ( $I_D = 15$ A, $T_J = 125^\circ\text{C}$ )	$V_{DS(on)}$	—	1.5 —	1.95 1.95	Vdc
Forward Transconductance ( $V_{DS} = 15$ Vdc, $I_D = 15$ Adc)	$g_{fs}$	10	—	—	mhos

**CURRENT SENSING CHARACTERISTICS**

Current Mirror Ratio (Cell Ratio) ( $R_{SENSE} = 0$ , $I_D = 15$ A, $V_{GS} = 10$ V)	n	900	—	960	—
Mirror Compliance Ratio ( $V_{GS} = 10$ Vdc, $I_D = 15$ Adc)	$K_{mc}$	—	0.65	—	—
Source Active Resistance ( $V_{GS} = 10$ Vdc, $I_D = 15$ Adc, $R_S = 10$ megohm)	$r_{a(on)}$	—	26	—	m $\Omega$
Mirror Active Resistance ( $V_{GS} = 10$ Vdc, $I_D = 15$ Adc)	$r_{m(on)}$	—	24	—	Ohms

**DYNAMIC CHARACTERISTICS**

Input Capacitance	$V_{DS} = 25$ V, $V_{GS} = 0$ $f = 1$ MHz	$C_{iss}$	—	—	1800	pF
Output Capacitance		$C_{oss}$	—	—	900	
Transfer Capacitance		$C_{rss}$	—	—	400	

**SWITCHING CHARACTERISTICS\***

Turn-On Delay Time	$V_{DD} = 30$ V, $I_D = 15$ A $R_{gen} = 50$ Ohms	$t_{d(on)}$	—	25	60	ns
Rise Time		$t_r$	—	110	200	
Turn-Off Delay Time		$t_{d(off)}$	—	120	200	
Fall Time		$t_f$	—	65	150	
Total Gate Charge	$V_{DS} = 64$ V, $I_D = 30$ A $V_{GS} = 10$ V	$Q_g$	—	62	75	nC
Gate-Source Charge		$Q_{gs}$	—	8	—	
Gate-Drain Charge		$Q_{gd}$	—	35	—	

**SOURCE-DRAIN DIODE CHARACTERISTICS\***

Forward On-Voltage	$I_S = 30$ A	$V_{SD}$	—	1.6	2	Vdc
Forward Turn-On Time		$t_{on}$	Limited by stray inductance			ns
Reverse Recovery Time		$t_{rr}$	—	200	—	

\*Indicates Pulse Test Pulse Width = 300  $\mu\text{s}$  max, Duty Cycle = 2%.

TYPICAL CHARACTERISTICS

Figure 1. On-Region Characteristics

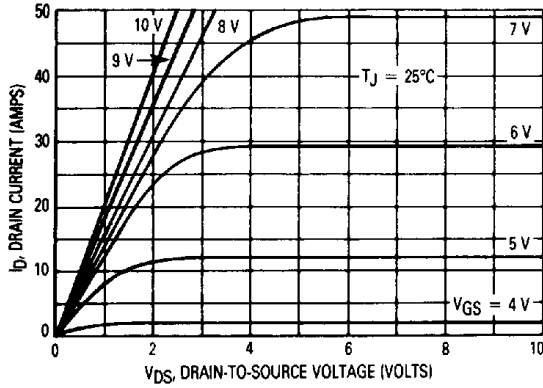


Figure 2. Gate Threshold Voltage Variation with Temperature

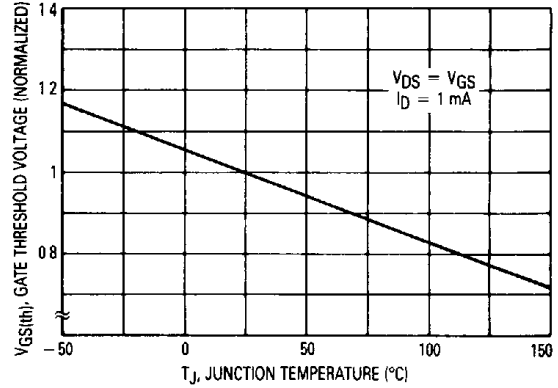


Figure 3. Transfer Characteristics

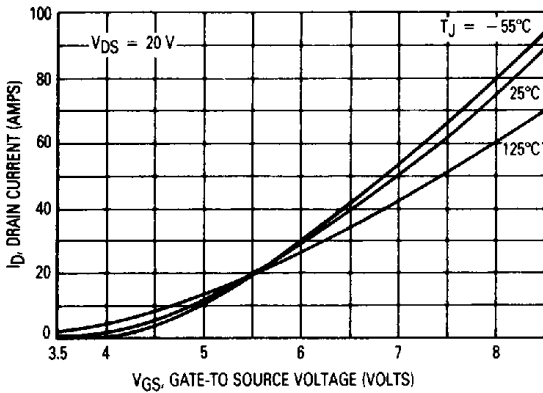


Figure 4. Stored Charge Variation

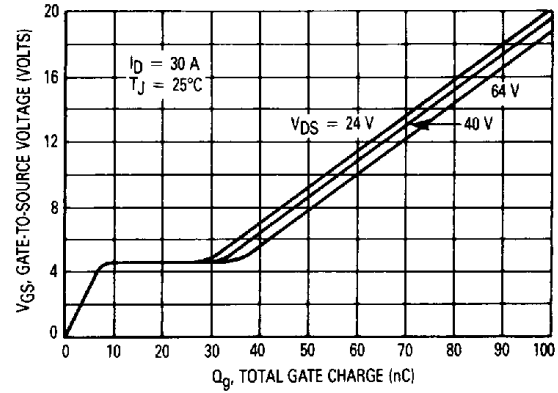


Figure 5. On-Resistance versus Drain Current

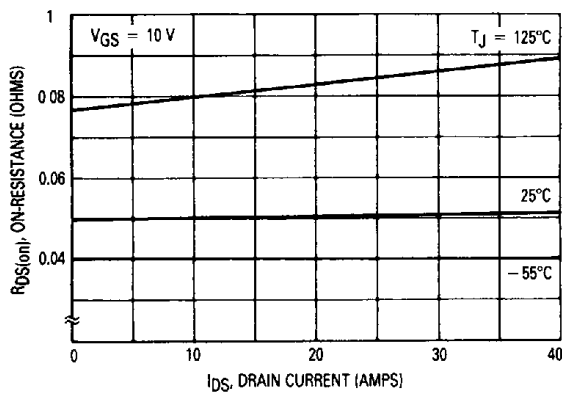
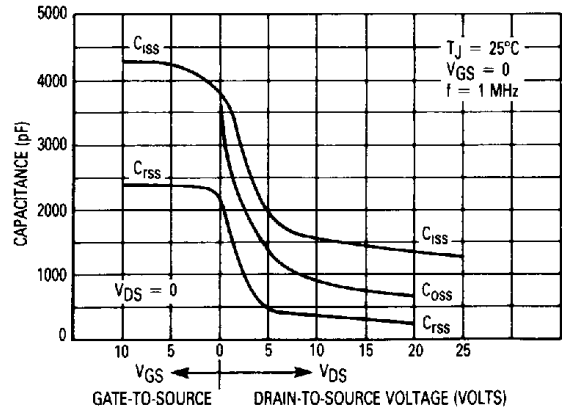
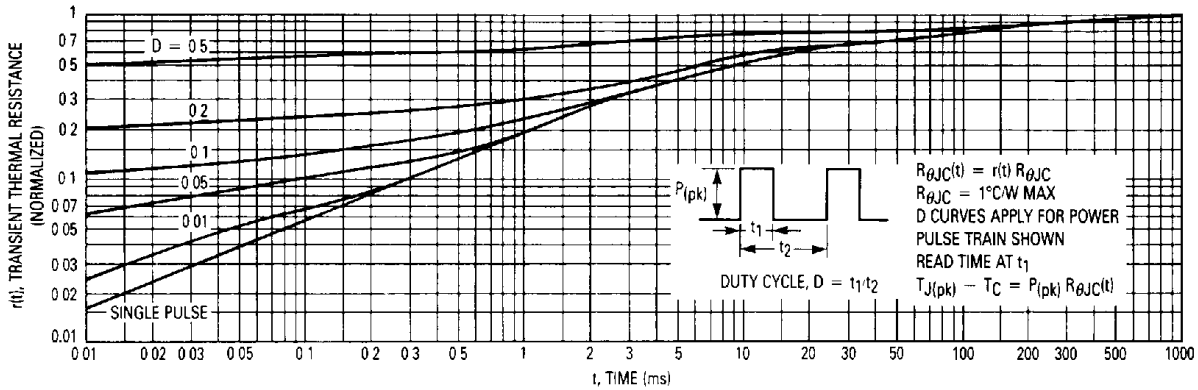


Figure 6. Capacitance Variation



TYPICAL CHARACTERISTICS

Figure 7. Thermal Response



SAFE OPERATING AREA INFORMATION

Figure 8. Maximum Rated Forward Biased Safe Operating Area

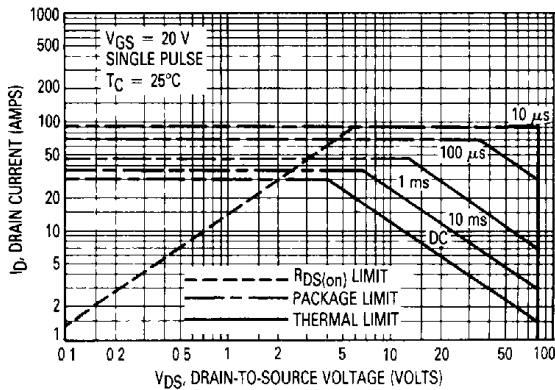
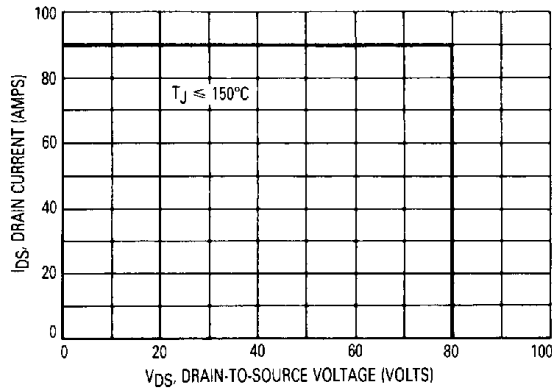


Figure 9. Maximum Rated Switching Safe Operating Area



FORWARD BIASED SAFE OPERATING AREA

The FBSOA curves define the maximum drain-to-source voltage and drain current that a device can safely handle when it is forward biased, or when it is on, or being turned on. Because these curves include the limitations of simultaneous high voltage and high current, up to the rating of the device, they are especially useful to designers of linear systems. The curves are based on a case temperature of  $25^\circ\text{C}$  and a maximum junction temperature of  $150^\circ\text{C}$ . Limitations for repetitive pulses at various case temperatures can be determined by using the thermal response curves. Motorola Application Note, AN569, "Transient Thermal Resistance-General Data and Its Use" provides detailed instructions.

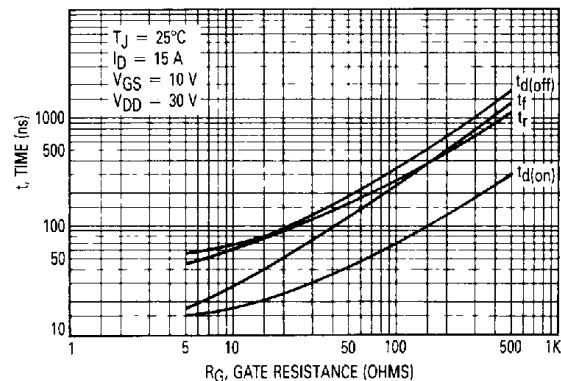
SWITCHING SAFE OPERATING AREA

The switching safe operating area (SOA) of Figure 9 is the boundary that the load line may traverse without incurring damage to the MOSFET. The fundamental limits are the peak current,  $I_{DM}$  and the breakdown voltage,  $V_{(BR)DSS}$ . The switching SOA shown in Figure 9 is applicable for both turn-on and turn-off of the devices for switching times less than one microsecond.

The power averaged over a complete switching cycle must be less than:

$$\frac{T_{J(max)} - T_C}{R_{\theta JC}}$$

Figure 10. Resistive Switching Time Variation with Gate Resistance



SAFE OPERATING AREA INFORMATION

Figure 11. On-Resistance Variation with Temperature

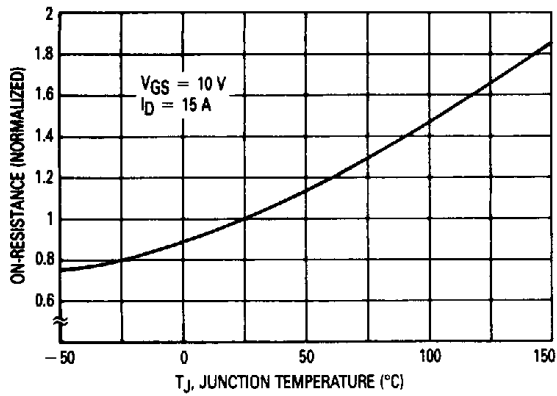


Figure 12. Breakdown Variation with Temperature

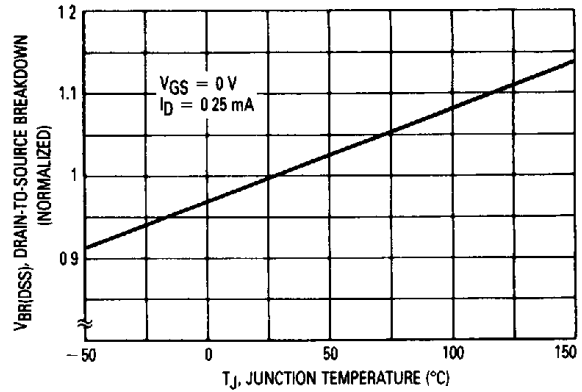


Figure 13. Sense Voltage Variation with Sense Resistance

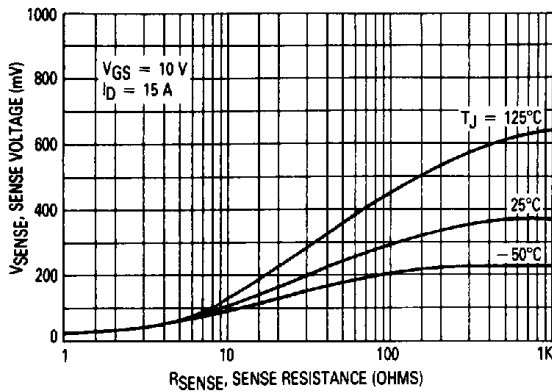


Figure 14. Sense Voltage Variation with Drain Current

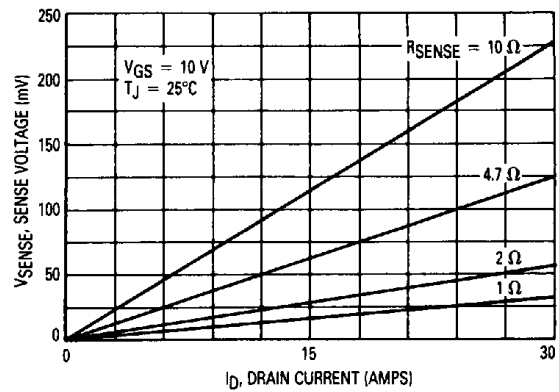


Figure 15. Sense Voltage Variation with Temperature

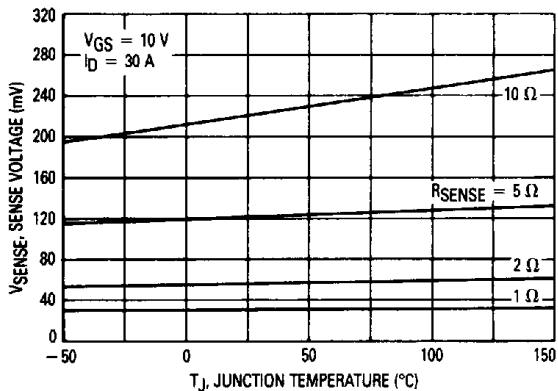


Figure 16. Sense Voltage Variation with Gate-to-Source Voltage

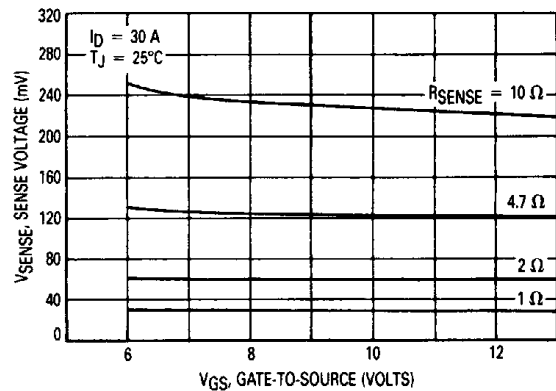


Figure 17. Current Mirror Ratio Variation with Drain Current

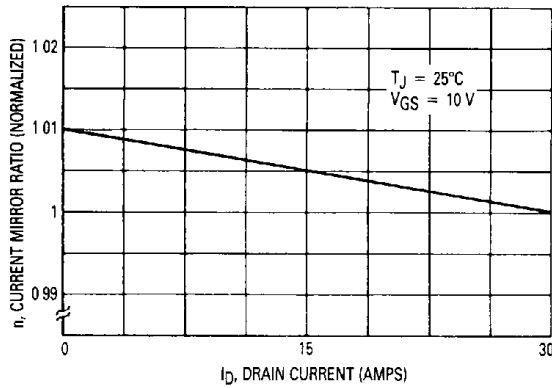


Figure 18. Current Mirror Ratio Variation with Gate-to-Source Voltage

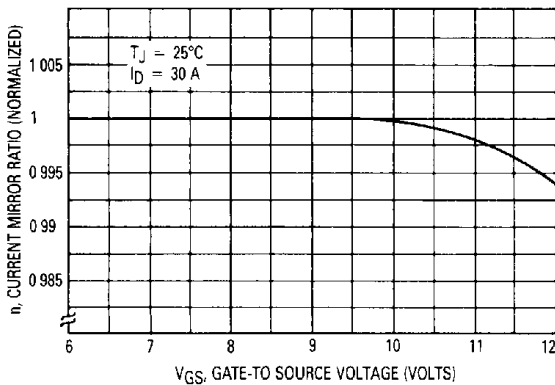
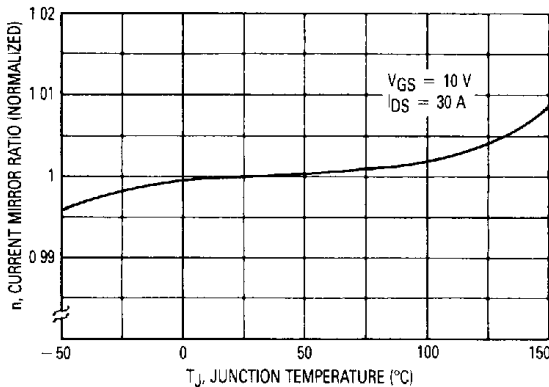


Figure 19. Current Mirror Ratio Variation with Temperature



LOSSLESS CURRENT SENSING

Assuming a fully switched on SENSEFET device, current sensing can be modeled with the simple resistor divider network shown in Figure 20. In this model,  $r_b$  is the bulk drain resistance,  $r_{m(on)}$  is the active mirror on-resistance,  $r_{a(on)}$  is the power section's active on-resistance and  $r_w$  is the source wire bond resistance. Using values for  $r_{a(on)}$  and  $r_{m(on)}$  from the electrical characteristics table;  $V_{SENSE}$ ,  $R_{SENSE}$ , and drain current may be calculated from the following sensing equations.

SENSING EQUATIONS:

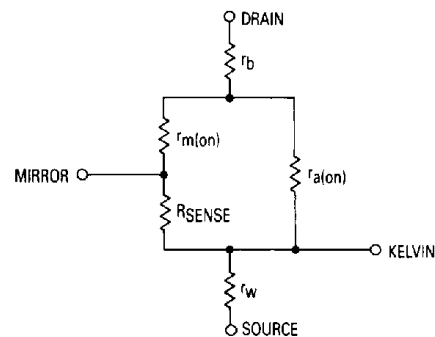
1.  $V_{SENSE} = I_D r_{a(on)} R_{SENSE} / (R_{SENSE} + r_{m(on)})$
2.  $R_{SENSE} = V_{SENSE} r_{m(on)} / (I_D r_{a(on)} - V_{SENSE})$
3.  $I_D = V_{SENSE} (R_{SENSE} + r_{m(on)}) / r_{a(on)} R_{SENSE}$
4.  $n = I_D / I_{SENSE}$ ; where  $R_{SENSE} = 0$
5.  $r_{a(on)} = r_{m(on)} / n$

When using these equations there are several factors to keep in mind.

They are described as follows:

- Maximum Sense Voltage: The maximum sense voltage that can appear at the mirror terminal is  $(r_{a(on)} / (r_{a(on)} + r_b) \times V_{DS(on)})$ . This ratio is called the mirror compliance ratio,  $K_{MCR}$ , and defines the upper boundary for sense voltage.
- Accuracy: Accurate current sensing is based upon the inherent matching of  $r_{m(on)}$  with the power section's active on-resistance,  $r_{a(on)}$ . When  $R_{SENSE} = 0$ , matching and current sensing accuracy are within  $\pm 3\%$ . As  $R_{SENSE}$  is increased, sensing accuracy is reduced since mirror current becomes dependent on the ratio of internal on-resistance to an external  $R_{SENSE}$ . From a practical point of view, relatively good sensing accuracy ( $\pm 10\%$ ) is maintained up to  $R_{SENSE} = r_{m(on)} / 2$ . As  $R_{SENSE}$  is increased beyond  $r_{m(on)}$ , sensing accuracy decreases rapidly.

Figure 20. SENSEFET Model



- **Ground Loop Errors:** Lossless current sensing is a technique that looks for 100 mV signals in a loop that may carry tens or even hundreds of amps. The potential for ground loop errors in this kind of an application is a first order design consideration. Internal wire bond resistance, contact resistance, and external wiring resistance are all significant. Therefore, it is important to reference sense voltage measurement circuitry to the Kelvin pin rather than power ground. In addition, referencing gate drive to the Kelvin pin rather than power ground will provide faster switching speeds.
- **Noise Suppression:** Switching noise is also a first order design issue. Layout, therefore, is critical. In addition, a single pole RC filter between  $R_{SENSE}$  and the current sensing circuitry's input terminals is often desirable. A  $1 \mu\text{sec}$  time constant is generally long enough to provide adequate noise suppression and short enough to provide adequate protection during overloads. An illustration is provided in Figure 21.
- **Double Pulse Suppression:** In PWM circuits it is critically important to include double pulse suppression in the control circuit topology. If the current limit loop is allowed to oscillate at its natural frequency, failure of the SENSEFET device is likely due to excessive power dissipation. By syncing current limiting to the clock with a latch, double pulse suppression architectures solve this problem, and provide effective protection from overload stress.
- **Parasitic Diode:** In addition to the power section's usual source-drain diode, there is a mirror-drain diode in the sense cells. Like the source-drain diode, the mirror-drain diode conducts during the reverse-mode operation, however, current sense characteristics are defined only in the forward-mode operation.
- **Reverse Recovery:** In bridge circuits, when a SENSEFET device's source-drain diode is commutated a voltage spike is produced at the mirror. This spike is short since it lasts only for the drain-source diode's reverse recovery time. However, its amplitude can be an order of magnitude larger than normal sense voltages and produce unwanted overcurrent trips. Blanking, filtering, or other suppression techniques may be required in some applications.

Figure 21. SENSEFET Device with Noise Suppression

